

# A NOVEL HYBRID RENEWABLE RESOURCES CONSTRUCTED WITH MULTILEVEL INVERTER USING SVM TECHNIQUE

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## ABSTRACT

*The proposed system presents power-control strategies of a grid-connected hybrid generation system with versatile power transfer. This hybrid system allows maximum utilization of freely available renewable energy sources like wind, fuel and photovoltaic energies. For this, an adaptive MPPT algorithm along with standard perturb and observes method will be used for the system.*

*The objective of this paper is to study a novel Multi level multistring inverter topology for DERs based DC/AC conversion system. In this study, a high step-up converter is introduced as a front-end stage to improve the conversion efficiency of conventional boost converters and to stabilize the output DC voltage of various DERs such as PV, Wind and fuel cell modules for use with the simplified newly constructed multilevel inverter. The proposed multilevel inverter requires only nine active switches instead of the twelve required in the conventional cascaded H- bridge (CCHB) multilevel inverter, control with SVM technique.*

*The inverter converts the DC output from non-conventional energy into useful AC power for the connected load. This hybrid system operates under normal conditions which include conventional and proposed cases of solar energy, fuel and wind energy. The proposed simulation results are presented to illustrate the operating principle, feasibility and reliability of this proposed system for Renewable resources.*

***Index Terms : DC/AC Power Conversion, Multilevel Inverter.***

## I. INTRODUCTION

NOWADAYS, photovoltaic (PV) energy appears quite attractive for electricity generation because of its noiseless, pollution-free, scale flexibility, and little maintenance. Because of the PV power generation dependence on sun irradiation level, ambient temperature, and unpredictable shadows, a PV-based power system should be supplemented by other alternative energy sources to ensure a reliable power supply. Fuel cells (FCs) are emerging as a promising supplementary power sources due to their merits of cleanness, high efficiency, and high reliability. Because of long startup period and slow dynamic response weak points of FCs

[1], mismatch power between the load and the FC must be managed by an energy storage system. Batteries are usually taken as storage mechanisms for smoothing output power, improving startup transitions and dynamic characteristics, and enhancing the peak power

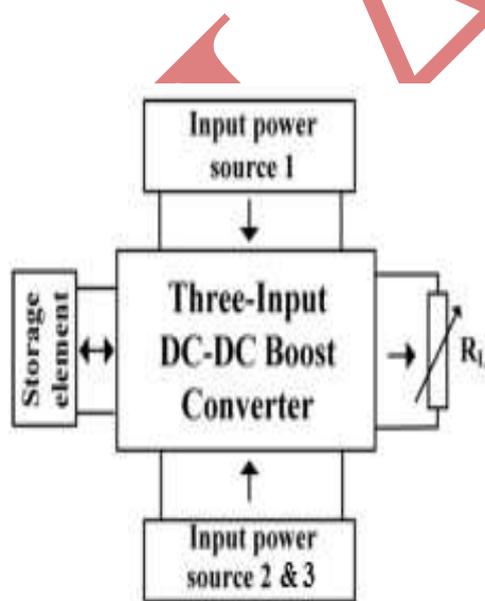
Capacity [2], [3]. Combining such energy sources introduces a PV/FC/battery hybrid power system. In comparison with single-sourced systems, the hybrid power systems have the potential to provide high quality, more reliable, and efficient power. In these systems with a storage element, the bidirectional power flow capability is a key feature at the storage port. Further input power sources should have the ability of supplying the load individually and simultaneously.

Many hybrid power systems with various power electronic converter have been proposed in the literature up to now. Traditional method that integrate different power sources to form a hybrid power system can be classified into AC coupled systems [4],[5] and ac-coupled systems [6]–[12]. However, the main shortcomings of these traditional integrating methods are complex system topology, high count of devices, high power losses, expensive cost, and large size. In recent years, several power conversion stages used in traditional hybrid systems are replaced by multi-input converters (MICs), which combine different power sources in a single power structure. These converters have received more attention in the literature because of providing simple circuit topology, centralized control, bidirectional power flow for the storage element, high reliability, and low manufacturing cost and size. In general, the systematic approach of generating MICs is introduced in [13], in which the concept of the pulsating voltage source cell and the pulsating current source cell is proposed for deriving MICs. One of the samples of these MICs is utilized in [14] to hybridize PV and wind power source in a unified structure. Besides, a systematic method to synthesize MICs is proposed in [15]. This paper deals with two types of MICs: in the first type, only one power source is allowed to transfer energy to the load at a time, and in the second type, all the input sources can deliver power to the load either individually or simultaneously. As another basic research in MICs, in [16] assumptions, restrictions, and conditions used in analyzing MICs are described, and then it lists some basic rules that allow determining feasible and un-feasible input cells that realize MICs from their single-input versions. Two multiple-input converters based on flux additively in a multi-winding transformer are reported in [17] and [18]. Because there was no possibility of bidirectional operating of the converter in [17], and complexity of driving circuits and output power limitation in [18], they are not suitable for hybrid systems. In [19], a three-port bidirectional converter with three active full bridges, two series resonant tanks, and a three-winding high-frequency transformer are proposed. In comparison with three-port circuits with only inductors and Diode Bridge at the load side, it gives higher boost gain and reduced switching losses due to soft-switching operation.

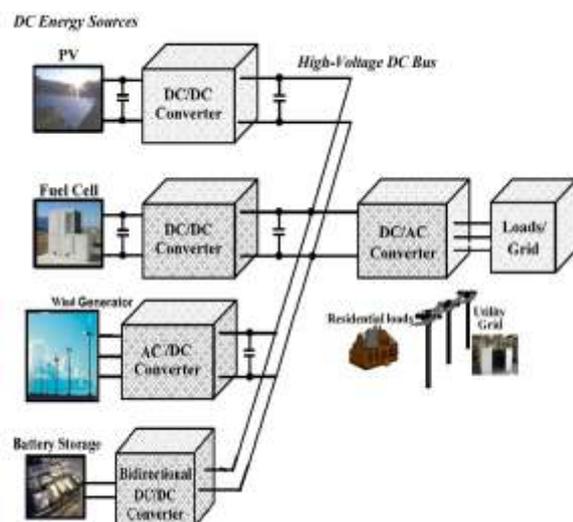
H. Tao et al. [20] present a family of multiport converters based on combination of dc link and magnetic coupling by utilizing half-bridge boost converters. The system features minimum number of conversion steps, low cost, and compact packaging. In [21], the input–output feedback control linearization for a DC–AC bidirectional MIC composing a high frequency isolating link transformer, two half-bridge boost converters at the input ports and a bidirectional cycloconverter at the output port is proposed. In [12]–[14], three MICs are proposed based on structure of the dc–dc boost converter. The dc–dc boost converter in [12] is useful for combining several energy sources whose power capacity or voltage levels are different. The multi input dc–dc converter proposed in [13] has the capability of operating in different converter topologies (buck, boost, and

buck–boost) in addition to its bidirectional operation and positive output voltage without any additional transformer. A three input dc–dc boost converter proposed by authors in [14] can combine a Wind, PV, an FC, and a battery in a simple unified structure. A comprehensive power management algorithm is realized in order to achieve maximum power point tracking (MPPT) of the PV source and set the FC in its optimal power operation range. A three port isolated full bridge topology is proposed in [3] for hybrid FC/battery system, which its aim is feeding a small autonomous load. This topology gains the advantage of bidirectional power flow due to the active full bridges in each port. Based on the model of the transformer reported in [3], the three transformer coupled half bridge converters proposed in [25] are analyzed. Thereby, phase-shift control method is used to manage the power flow among the three ports in addition to soft switching for all switches over a wide input range.

Wai et al. presents two kinds of MICs in [2] and [16]. a high step-up ratio bidirectional MIC with high efficiency is proposed. The converter operates in standalone state, united power supply state, and charge and discharge states. A two input power converter for a hybrid FC/battery power system is proposed in [2] with zero voltage switching characteristic. Although the circuit efficiency is greatly developed, the converter does not provide bidirectional functionality and is not able to boost the input voltage to a higher level. Moreover, the summation of duty ratios should be greater than 1 and the two input voltages should be in the same level in the dual power supply operation state. Qian et al. presents a hybrid power system consist of a PV and a battery for satellite applications, and a four port hybrid power system supplied by a PV, a wind, and a battery ,a power control strategy is designed to manage the charge balance of the battery in order to regulate the output voltage. In these systems, the PV and the wind sources are exploited in MPPT conditions. Moreover, control strategies of the both systems are designed based on small signal modeling of the converters. Proper decoupling method is productively introduced to separately design compensators for cross coupled control loops.



**Fig.1 Proposed system overview.**



**Fig.2 Configuration of multi string inverter for Various DERs application.**

In this paper, a new four input dc–dc boost converter is proposed for hybrid power system applications. As shown in Fig. 1, the proposed converter interfaces three unidirectional ports for input power sources, a bidirectional port for a storage element, and a port for output load in a unified structure. The converter is current source type at the both input power ports and is able to step up the input voltages. The proposed structure utilizes only four power switches that are independently controlled with four different duty ratios. Utilizing these duty ratios facilitates controlling the power flow among the input sources and the load. Powers from the input power sources can be delivered to the load individually or simultaneously.

## II. POWER CONTROL TECHNIQUES FOR CONVERTER STAGES

### 2.1 High Power Converter Stage

In this study, high Power converter topology in [26] is introduced to boost and stabilize the output DC voltage of various DERs such as PV, Wind and fuel cell modules for employment of the proposed simplified multilevel inverter. The architecture of a high power converter initially introduced from [26], depicted in Fig. 7, and is composed of different converter topologies: boost, flyback, and a charge pump circuit.

The coupled inductor of the high power converter in Fig. 7 can be modeled as an ideal transformer, a magnetizing inductor, and a leakage inductor. According to the voltage seconds balance condition of the magnetizing inductor the voltage of the primary winding can be derived as

$$v_{pri} = v_{in} \cdot D / (1 - D) \quad (1)$$

Where  $v_{in}$  represents each the low-voltage DC energy input sources, and voltage of the secondary winding is

$$v_{sec} = \frac{N_s}{N_p} \cdot v_{pri} = \frac{N_s}{N_p} \cdot v_{in} \cdot D / (1 - D) \quad (2)$$

Similar to that of the boost converter, the voltage of the charge-pump capacitor  $C_{pump}$  and clamp capacitor  $C_c$  can be expressed as

$$v_{cp} = v_{Cc} = v_{in} \cdot 1 / (1 - D) \quad (3)$$

Hence, the voltage conversion ratio of the high step-up converter, named input voltage to bus voltage ratio, can be derived as [26]

$$\frac{v_{si}}{v_{in}} = \left( 2 + \frac{N_s}{N_p} \cdot D / (1 - D) \right) \Big|_{i=1,2} \quad (4)$$

### 2.2 Simplified Multilevel Inverter Stage

To assist in solving problems caused by cumbersome power stages and complex control circuits for conventional multilevel inverters, this work reports a new three-phase multi string topology, presented as a new basic circuitry in Fig. 3.

Referring to Fig. 7, it should be assumed that, in this configuration the three capacitors in the capacitive voltage divider are connected directly across the DC bus, and all switching combinations are activated in an output cycle. The dynamic voltage balance between the two capacitors is automatically controlled by the preceding high step-up converter stage. Then, we can assume  $V_{S1}=V_{S2}=V_{S3}=V_s$ .

This topology includes nine power switches—three fewer than the CCHB inverter with twelve power switches - which drastically reduces the power circuit complexity and simplifies modulator circuit design and implementation. The PD PWM control scheme is introduced to generate switching signals and to produce five output-voltage levels: zero,  $V_s$ ,  $2V_s$ ,  $-V_s$ , and  $-2V_s$ .

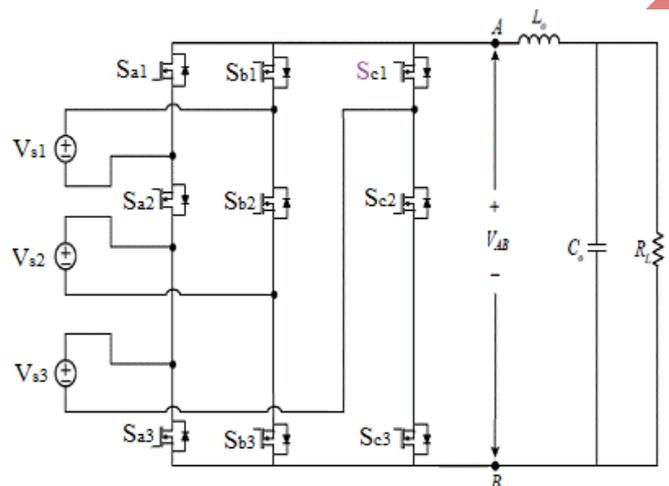


Fig.3. Basic Seven-Level Inverter Circuitry.

This inverter topology uses two carrier signals and one reference to generate PWM signals for the switches. The modulation strategy and its implemented logic scheme in Fig.4 is a widely used alternative for phase disposition modulation. With the exception of an offset value equivalent to the carrier signal amplitude, two comparators are used in this scheme with identical carrier signals  $V_{tri1}$  and  $V_{tri2}$  to provide high-frequency switching signals for switches  $S_{a1}$ ,  $S_{b1}$ ,  $S_{a3}$  and  $S_{b3}$ . Another comparator is used for zero crossing detection to provide line-frequency switching signals for switches  $S_{a2}$  and  $S_{b2}$ .

For convenient illustration, the switching function of the switch in Fig. 3 is defined as follows

$$S_{aj} = \begin{cases} 1, & S_{aj} \text{ ON} \\ 0, & S_{aj} \text{ OFF} \end{cases} \quad j=1, 2, 3 \quad (5)$$

$$S_{bj} = \begin{cases} 1, & S_{bj} \text{ ON} \\ 0, & S_{bj} \text{ OFF} \end{cases} \quad , j = 1,2,3 \quad (6)$$

$$S_{c_j} = \begin{cases} 1, & S_{c_j} \text{ ON} \\ 0, & S_{c_j} \text{ OFF} \end{cases} \quad , j = 1,2,3 \quad (7)$$

Table I. lists switching combinations that generate the required seven output levels. The corresponding operation modes of the multilevel inverter stage are described clearly as follows.

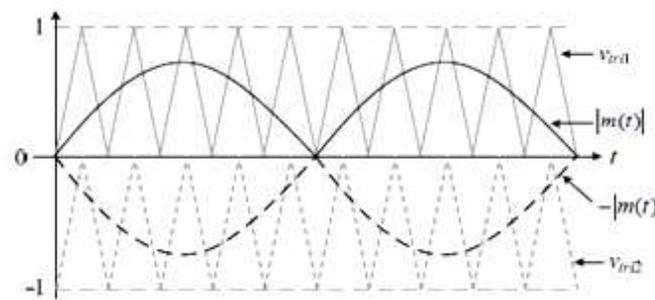


Fig.4 Modulation Strategy: Carrier/Reference Signals

Table-1  
Switching Combinations

S <sub>a1</sub>	S <sub>a2</sub>	S <sub>a3</sub>	S <sub>b1</sub>	S <sub>b2</sub>	S <sub>b3</sub>	S <sub>c1</sub>	S <sub>c2</sub>	S <sub>c3</sub>	V <sub>AB</sub>
0	1	0	1	0	1	0	0	1	2V <sub>s</sub>
0	1	1	1	0	0	0	1	1	V <sub>s</sub>
1	1	0	0	0	1	1	1	1	V <sub>s</sub>
1	1	1	0	0	0	0	0	0	0
0	0	0	1	1	1	1	0	0	0
1	0	0	0	1	1	0	0	1	-V <sub>s</sub>
0	0	1	1	1	0	1	0	1	-V <sub>s</sub>
1	0	1	0	1	0	1	1	0	-2V <sub>s</sub>

To verify the feasibility of the three-phase seven-level inverter, a widely used software program PSIM is applied to simulate the circuit according to the previously mentioned operation principle. The control signal block is shown in Fig. 4.  $m(t)$  is the sinusoidal modulation signal. Both  $V_{tri1}$  and  $V_{tri2}$  are the two triangular carrier signals. The peak value and frequency of the sinusoidal modulation signal are given as  $m_{peak}=0.7$  and  $f_m=60\text{Hz}$ , respectively. The peak-to-peak value of the triangular modulation signal is equal to 1, and the switching frequency  $f_{tri1}$  and  $f_{tri2}$  are both given as 1.8kHz.

The three input voltage sources feeding from the high step-up converter is controlled at 100V, i.e.  $V_{s1}=V_{s2}=V_{s3}=100\text{V}$ . The simulated waveform of the phase voltage with seven levels is shown in Fig. 5. The switch voltages of  $S_{a1}$ ,  $S_{a2}$ ,  $S_{a3}$ ,  $S_{b1}$ ,  $S_{b2}$ ,  $S_{b3}$ ,  $S_{c1}$ ,  $S_{c2}$  and  $S_{c3}$  are all shown in Fig. 6.

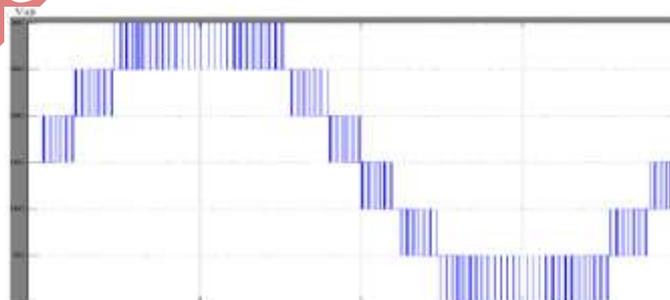
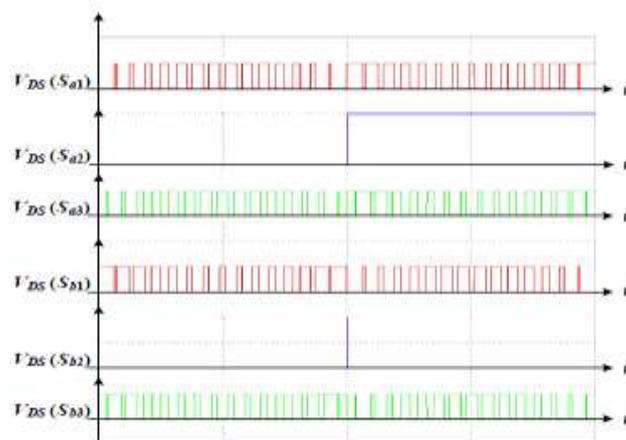


Fig.5 simulated waveforms of phase voltage  $V_{AB}$  of inverter stage [Scale: 100V/div]



**Fig.6. simulated waveforms of switch voltage for inverter stage with in a line period [Scale: 100V/div]**

The average switching power loss  $P_s$  in the switch caused by these transitions can be defined as

$$P_s \approx 0.5V_{DS} I_o f_s [t_c (on) + t_c (off)] \quad (8)$$

Where  $t_c (on)$  and  $t_c (off)$  are the turn-on and turn-off crossover intervals, respectively;  $V_{DS}$  is the voltage across the switch; and  $I_o$  is the entire current which flows through the switch. The voltage stresses of the nine switches of the CCHB inverter are all equal to  $V_s$ .

For simplification, both the proposed circuit and CCHB inverter are operated at the same turn-on and turn-off crossover intervals and at the same load  $I_o$ . Then, the average switching power loss  $P_s$  is proportional to  $V_{DS}$  and  $f_s$  as

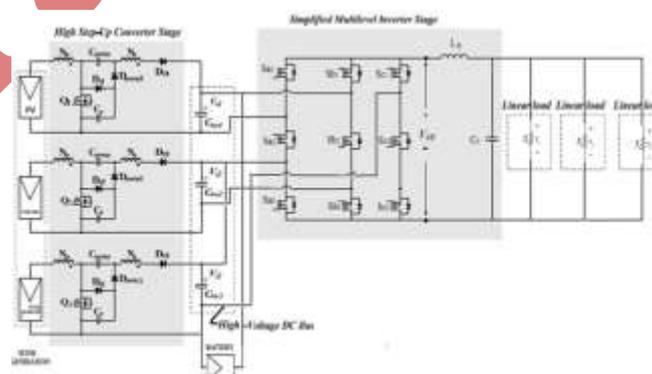
$$P_s \propto V_{DS} \cdot f_s \quad (9)$$

According to Eq. (9) the switching losses of the CCHB inverter from twelve switches can be, obtained as

$$P_{s, H\text{-bridge}} \propto 8V_s f_s \quad (10)$$

Similarly, the switching power loss of the proposed three phase seven-level inverter due to nine switches can also be obtained as

$$P_{s, proposed} \propto 4V_s f_s + 2(2V_s) f_m \propto 4V_s (f_s + f_m) \quad (11)$$



**Fig.7. Multi-level inverter topologies of CCHB inverter [15]**

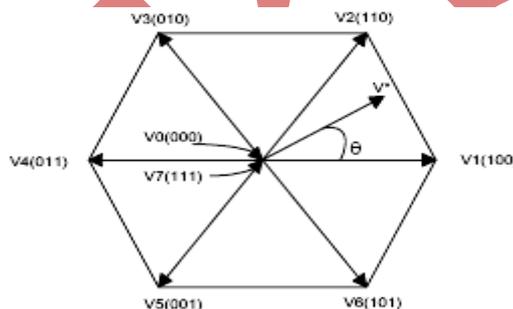
Because switches  $S_{a2}$ ,  $S_{b2}$  can only be activated twice in a line period (60Hz) and the switching frequency is larger than the line frequency ( $f_s \gg f_m$ ), the switching losses of the proposed circuit is approximated to  $4V_s f_s$ , obviously, the switching power loss is nearly half that of the CCHB inverter.

Considering the harmonics in the inverter output voltage  $V_{AB}$ , the amplitude of the fundamental and harmonic components in the output voltage  $V_{AB}$  are calculated by MATLAB software. The phase shift SVM technique is adopted for the CCHB Inverter. the CCHB multilevel inverter is operated in the same condition, including the same switching frequency 18kHz and modulation index, the same input voltage  $V_S=100V$  and output L-C filter,  $L_o=1mH$ ,  $C_o=4.7\mu F$ .

### 2.3 Dc-Ac Power Converter Space Vector Modulation Technique.

Nine power switches of inverter with 8 possible combinations shown in "Figure. 7" are corresponding to effective voltage space vector  $U_1 - U_9$  and 2 zero vector  $U_0, U_9$ . The phase angle between one effective voltage space vector and adjacent one is 40 degrees. They constitute 9 uniform segments. The three digits in brackets express the linking state between three-phase output A,B,C and the input DC, such as  $M=101$  which represents the switching of the switches  $S_{a1}, S_{b1}$  and  $S_{c1}$ .

The output voltage space vectors and the corresponding switching states are represented in "Fig. 8".



**Fig.8.The Composition Of Output Voltage Vector and Switching Stages.**

Any expected output voltage space vector  $U_j$  is formed by adjacent two basic output voltage vectors  $U_M, U_N$ ,  $U_z$  and zero output voltage  $U_0$  or  $U_9$ . Suppose the angle between  $U_j$  and  $U_M$  is  $\theta_j$ .

$$U_j = d_M U_M + d_N U_N + d_0 U_0 \quad (12)$$

Where  $d_M, d_N$  and  $d_0$  are the ratio cycles of  $U_M, U_N$  and  $U_0$  respectively. And

$$d_M = T_M / T_\delta = m_v \sin(60^\circ - \theta_j) \quad (13)$$

$$d_N = T_N / T_\delta = m_v \sin(\theta_j) \quad (14)$$

$$d_0 = 1 - d_M - d_N \quad (15)$$

Where  $T_M, T_N$  is the switching time of vectors  $U_M$  and  $U_N$  respectively.  $T_\delta$  is the switching period of PWM.  $m_v$  is the modulation index of output voltage. And

$$m_v = (2/3)^{1/2} U_{om} / (U_{im} m_c \cos \phi) \quad (16)$$

Where  $U_{om}$  and  $U_{im}$  are the amplitude of output and input voltage,  $m_c$  is the input current modulation index, generally set  $m_c = 1$ ,  $\phi$  is the input power factor angle. When the rotating space vector  $U_j$  locates in a segment, the local average of output voltage can be formed by two adjacent basic voltage space vectors constituting this segment and one zero voltage space vector.

### 2.4 SVM Techniques

A different approach to SPWM is based on the space vector representation of voltages in the d, q plane. The d, q components are found by Park transform, where the total power, as well as the impedance, remains unchanged. Fig.9 space vector shows space vectors in according to 9 switching positions of inverter,  $V^*$  is the phase-to-center voltage which is obtained by proper selection of adjacent vectors  $V1$  and  $V2$ .

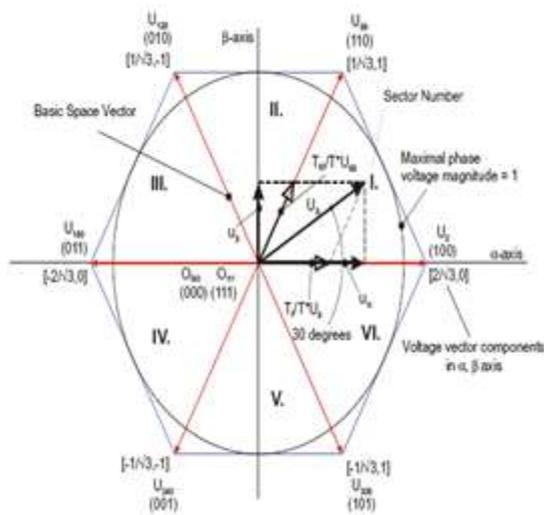


Fig.9. Inverter Output Voltage Space Vector

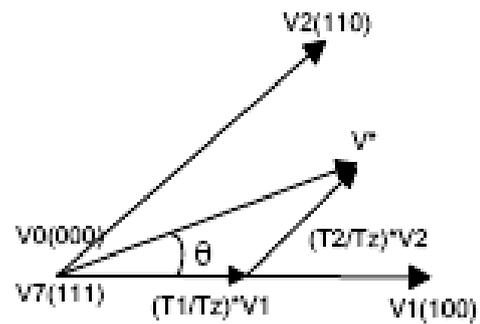


Fig 9.1 Determination of Switching Times

The reference space vector  $V^*$  is given by Equation (17), where  $T1$ ,  $T2$  are the intervals of application of vector  $V1$  and  $V2$  respectively, and zero vectors  $V0$  and  $V7$  are selected for  $T0$ .

$$V^* T_z = V1 * T1 + V2 * T2 + V0 * (T0/2) + V7 * (T0/2) \dots \dots \dots (17)$$

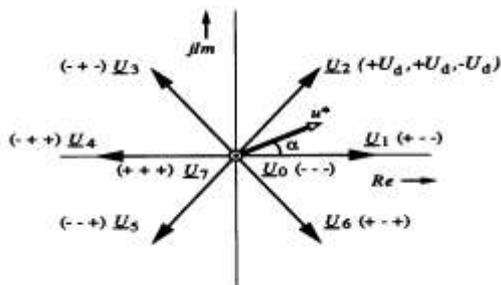


Fig 9.2 Space Vector Modulation

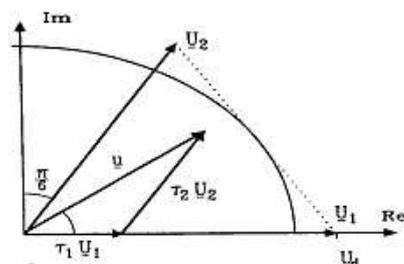


Fig.9.3 Definition of the Space Vector

The amplitude of  $u_0$  and  $u_9$  equals 0. The other vectors  $u_1 \dots u_9$  have the same amplitude and are 40 degrees shifted. By varying the relative on-switching time  $T_{on}$  of the different vectors, the space vector  $u^*$  and also the output voltages  $u_a$ ,  $u_b$  and  $u_c$  can be varied and is defined as:

$$\begin{aligned} u_a &= \text{Re} ( u^* ) \\ u_b &= \text{Re} ( u^* \cdot a^{-1} ) \\ u_c &= \text{Re} ( u^* \cdot a^{-2} ) \end{aligned} \dots\dots\dots(18)$$

During a switching period  $T_{on}$  and considering for example the first sector, the vectors  $u_0$ ,  $u_1$  and  $u_2$  will be switched on alternatively.

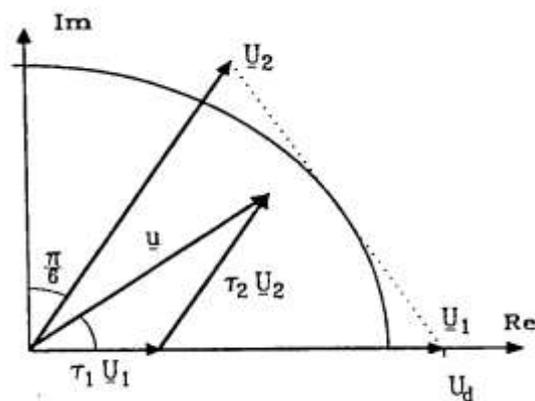


Fig.9.3 Definition of the Space Vector

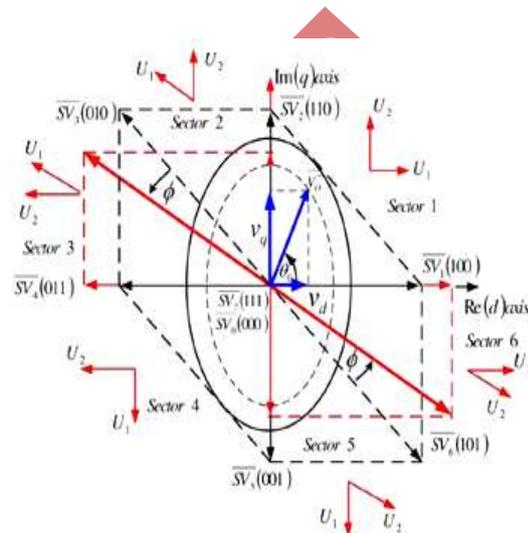


Fig 9.4. SVM Vector Diagram for New Switching Converter

Depending on the switching times  $t_0$ ,  $t_1$  and  $t_2$  the space vector  $u^*$  is defined as:

$$\begin{aligned} u^* &= 1/T_{on} \cdot (t_0 \cdot u_0 + t_1 \cdot u_1 + t_2 \cdot u_2) \\ u^* &= t_0 \cdot u_0 + t_1 \cdot u_1 + t_2 \cdot u_2 \\ u^* &= t_1 \cdot u_1 + t_2 \cdot u_2 \end{aligned} \dots\dots\dots(19)$$

Where

$$t_0 + t_1 + t_2 = T_{on} \text{ and}$$

$$t_0 + t_1 + t_2 = 1$$

$t_0$ ,  $t_1$  and  $t_2$  are the relative values of the on witching times. They are defined as:  $t_1 = m \cdot \cos (a + p/6)$ ,

$$t_2 = m \cdot \sin a \quad t_0 = 1 - t_1 - t_2$$

Their values are implemented in a table for a modulation factor  $m = 1$ . Then it will be easy to calculate the space vector  $u^*$  and the output voltages  $u_a$ ,  $u_b$  and  $u_c$ . The voltage vector  $u^*$  can be provided directly by the optimal vector control laws  $w_1$ ,  $v_{sa}$  and  $v_{sb}$ . In order to generate the phase voltages  $u_a$ ,  $u_b$  and  $u_c$  corresponding to the desired voltage vector  $u^*$  the above SVM strategy is proposed.

### III SIMULATION RESULTS

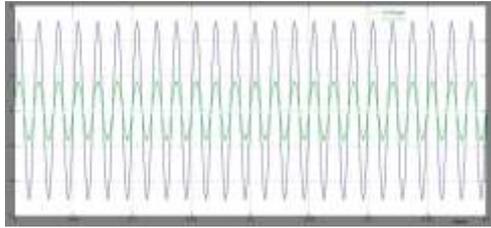


Fig.10 Output Voltage and Current with Unity Power factor

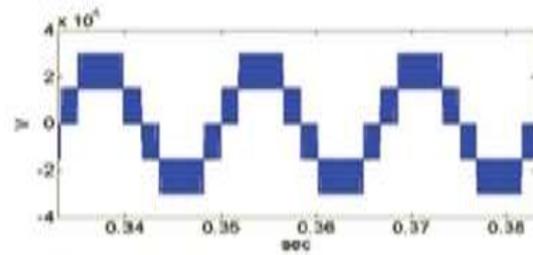


Fig.11 Inverter Output Five Level Voltage

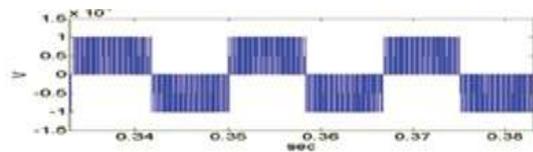


Fig.12 Inverter line voltage

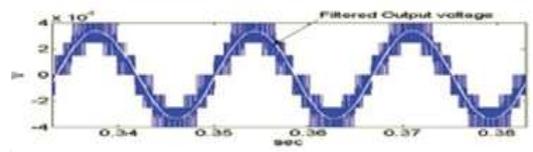


Fig.13 Inverter Output Seven Level Voltage

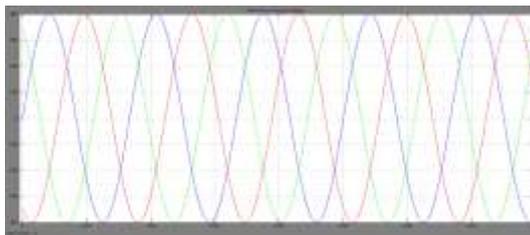


Fig.14 Load voltage with LC filters



Fig.15 Load Current with Lc filters wave forms

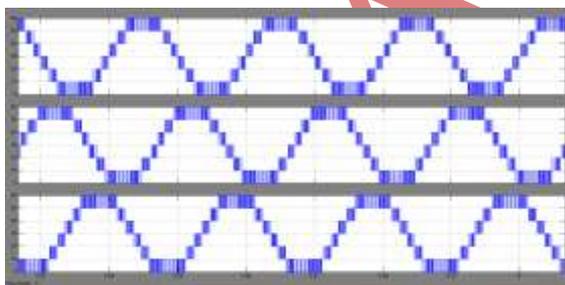


Fig.16 Three Phase A,B& C Multi level of Renewable power Inverter wave forms

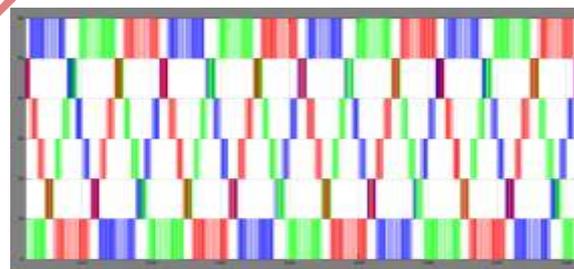


Fig.17 Three Phase Multi level of Renewable power Inverter Voltage with PLL Block Wave Forms

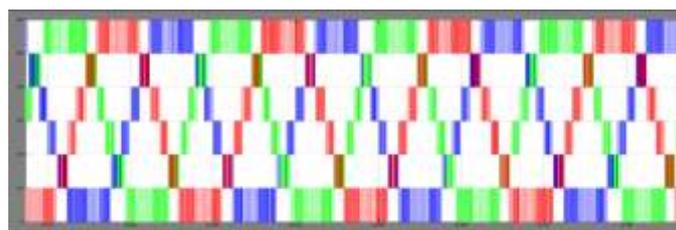


Fig.18 Three Phase Multi Level of Renewable Power Inverter Current with PLL Block Wave Forms

**Table II**  
**Components Parameters of the Proto Type**

High Step DC/DC Converter Stage		
Components	Symbol	Value/Part no.
Coupling inductor	$L_m$ , NP:NS	24 $\mu$ H, ETD 39,NP:NS = 1.5
Power switches	$Q_1, Q_2, Q_3$	FDB3632,(100V, 9m $\Omega$ )
Charge-pump diodes	$D_{pump1}, D_{pump2}, D_{pump3}$	STPS10AH100,(100V, 10A)
Clamping diodes	Dc1, Dc2, Dc3	STPS10AH100,(100V, 10A)
Output diodes	$D_{O1}, D_{O2}$	15ETH06S,(600V, 12A)
Charge-pump caps	$C_{pump}$	2 $\times$ 4.7 $\mu$ F/630V
Bus capacitors	$C_{bus1}, C_{bus2}, C_{bus3}$	2000 $\mu$ F/400V
Simplified Multilevel DC/AC stage		
Power switches	$S_{a1}, S_{a2}, S_{a3}, S_{b1}, S_{b2}, S_{b3}$ $Sc1, sc2, sc3$	FDB2710,(250V, 2.5m $\Omega$ )
Output inductor	$L_o$	1mH
Output capacitor	$C_o$	4.7 $\mu$ F/630V

#### IV. CONCLUSIONS

The proposed system illustrates Renewable & Sustainable power generation strategies of a grid system with versatile power transfer. This grid system allows maximum utilization of freely available renewable energy sources like fuel cell, WTG and photovoltaic energies. For this, an adaptive MPPT algorithm along with standard perturb and observes (P&O) method will be used for the Wind, PV & Fuel system with DC/AC Power Converter with SVM Technique.

Also, this configuration allows the sources to supply the load separately or simultaneously depending on the availability of the energy sources. The turbine rotor speed is the main determinant of mechanical output from wind turbine to Permanent Magnet Synchronous Generator (PMSG) is coupled for attaining energy conversion system. Renewable energy resources like Fuel cell and Solar cell power generated are interconnected to DC Link. The inverter converts the DC output from non-conventional energy into useful AC power for the connected load (Industrial & Commercial Loads). This Grid system operates under normal conditions which include normal room temperature or At Any atmospheric Condition. This work reports a newly-constructed three-phase multi string multilevel inverter topology that produces a significant reduction in the number of power devices required to implement multilevel output for DERs. The studied inverter topology with SVM Technique offer strong advantages such as improved output waveforms, smaller filter size, and lower EMI. Total harmonic distortion (THD) of the voltage and current at the output of the Conventional inverter THD =1.45 and Proposed CCHB multi-level inverter THD= 0.54. Simulation results show the effectiveness of the proposed solution. The Proposed simulation results are analyzed to illustrate the operating principle, feasibility

and reliability of this proposed grid systems.

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